

Model A-15B
Audio Console



TECHNICAL MANUAL

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5851 FLORIN-PERKINS ROAD SACRAMENTO, CALIFORNIA 95828

A DIVISION OF COMPUTER EQUIPMENT CORPORATION

A-15B CONSOLE

SPECIFICATIONS

MIXERS:	Five
INPUTS:	Fourteen Total; Two each for mixers 1 to 4, six for mixer five.
INPUT LEVELS:	Low-level; -55 dbm nominal from 50 or 150/250 ohms. Low-level preamps standard on mixer one. Optional for mixers two through five. High level; minus 10dbm nominal. Standard on mixers two to five. Optional for Mixer one. Note: High-level inputs are 10K transformer bridging. Refer to general description.
OUTPUTS:	Program, monitor, cue, phones and P.A.
OUTPUT LEVELS:	Program; 8dbm/600 ohms at 0 VU. 22dbm max. Monitor; 8 w/8 ohms (4-16 ohms). Cue; 1 w/3.2 or 4 ohms. P.A.; 1 v. nominal into 10,000 ohm.
RESPONSE:	All outputs; -2db, 20Hz to 20 kHz.
NOISE:	Below 65db at 0 vu out with -55dbm low level input (20-20kHz). Below 75db at 0 vu out with -10dbm hi-level input (20-20 kHz.).
DISTORTION:	Prog. and Aud: Less than 0.5% THD at 8dbm out. Monitor and Cue; Less than 1% THD at rated output

CROSSTALK: Within 6db of noise

POWER: 117/234 vac, 50/60 Hz.

DIMENSIONS: Width 15", Height 6 3/4", Depth 11 1/2" (Overall)

SHIPPING
WEIGHT: 26 lbs.

MUTING: Three internal relays operate from mixers 1, 2 or 3 in any combination via internal patch-panel. Each relay provides independent muted Monitor Out plus isolated closure for control of external equipment (117 vac, 5A max).

See description for added details.

A-15B CONSOLE

DESCRIPTION

GENERAL: The A-15B is a desk-type audio console featuring five mixing channels with selection of A and B inputs for all mixers. In addition, mixer five has a five push-button pre-selector for the B input. As normally supplied the first mixer includes a low-level microphone preamplifier and the remaining four are high-level inputs. The high-level and low-level boards are interchangeable and can be installed in any combination. The input impedance of high-level channels is 10K ohms transformer-coupled balanced, which avoids loading the source and greatly increases the flexibility of the console. This also permits the console to be driven from sources that are not designed to work into a 600 ohm load. In the occasional instance where a 600 ohm termination is required, it is a simple matter to add a 620 ohm resistor across the line at either the source or console end. Alternately, provision is made on the transformer input board for addition of this resistor, in which case performance is identical to earlier consoles but termination is then effective only on the input line being selected by the console

MUTING PROVISIONS: Three separate relays are provided, each controlling an independent MONITOR OUT speaker terminal, while a fourth terminal allows uninterrupted monitoring. Also, each relay provides an isolated closure via a male Jones connector for direct control of external equipment such as On-the-Air lamps, Turntables or Cartridge Equipment. Relay control is determined by

connections made on the relay board, and each relay may be connected so as to close from any combination of pre-selected inputs on mixers one through three, in each case the relay(s) will activate when the mixer selector switch is thrown to the A or B position and released in the center Off position.

A-15B PARTS LIST

For Components Mounted on PC Boards, Refer to Individual PC Board Schematic

Potentiometers	# Required	Sparta #
Mixer w/cue switch	5	130-0021
Monitor gain w/power sw.	1	130-0021
Master Gain	1	130-0022
Cue Gain	1	130-0022
Headphone gain	1	130-0022
P.A. Gain	1	130-0022
Switches		
A-B Selector	5	299-0001
5 "B" input selector	1	296-0021
"Aux" selector	1	296-0021
"VU" Meter	1	368-0007
Output Transformer	1	318-0014
Input Connectors		
Barrier Strip	3	477-0022
Mic Socket	2	396-0027
Knobs		
Mixers	5	550-0011
Monitor/master/phones/cue	4	550-0001
A/B Selector	5	550-0019
"5B"/Aux input	10	550-0015
Fuse 1/4 ASB (in PS-6 Supply)	1	261-0010

AUDIO CONSOLE

INSTALLATION

GENERAL: Most input and output connections are made via rear-panel barrier strips. Spade lugs or fanning-strips are not required since the barrier strips are designed with captive plates to easily accommodate several stripped wires per terminal, either solid or stranded. Rear panel connections are all clearly identified to facilitate installation without resorting to the manual or to a numbered diagram.

Audio connections are normally made with twisted-pair, shielded cable such as Belden 8737 (stranded) or 8739 (solid). Either may be used, although it is generally more satisfactory to use solid wire in a permanent installation where flexibility is not required, since solid wire is easier to handle and less apt to inadvertently short to an adjacent terminal. Single-ended outputs and inputs can use the same cable by simply clipping off the unused conductor.

Both the high-level and low-level inputs are brought to isolated balanced input transformers. The input terminals include a ground connection for the cable shield and the transformer input windings are ungrounded, or "floating". This prevents the possibility of setting up a severe ground-loop and also permits one side of the transformer input to be grounded for single-ended operation if desired. In like manner, the program line output is also isolated.

A central ground lug is provided on the rear panel for connection to the system master ground, and as heavy a gage strap or braid as practical should be used.

Once the desired input and output audio connections are made, it is only necessary to complete the power connections, set the master and monitor gain controls to suitable levels and turn the console on. As a general rule, normal operating position for all level controls will be at approximately 10 o'clock. There is considerable reserve gain available in the program line amplifier and it is usually not advisable to turn both Master and Mixer gain controls to full clockwise at the same time. No harm will come from abnormal control settings, but the possibility would exist for decreased signal-to-noise ratio or increased distortion.

MONITOR AND CUE AMPS: The monitor and cue amplifiers are rated for an 8 ohm load, although they will operate equally well with a 4 ohm load. (or two 8 ohm speakers in parallel) with slightly increased power output capability. If the load is higher than 8 ohms, power output will be reduced accordingly since a given voltage level will then produce less current.

Both amplifiers are a direct-coupled transformerless design and do not require termination in the absence of a load. The load should never be less than 4 ohms, however, and if multiple speakers are to be used, it may be necessary to consider a series-parallel arrangement to provide 4 ohm minimum loading. A short circuit should be avoided at all costs.

When connecting speakers, it should be considered that eight watts RMS into 8 ohms requires a peak audio current of 1.4 amps. It is suggested that for moderate to long runs, an 18 gauge cable pair such as common, lamp or "zip-cord" be used to avoid power loss on audio peaks.

MUTING: As indicated in the General Description, the muting system is quite flexible. No external connections need be made other than to connect the speakers to the proper terminals as indicated on the rear panel. Jumpers must be connected internally on the relay board to activate the relays as required for the particular application. Each relay coil terminates at an eyelet with a short jumper wire attached and the relay will close if this wire is grounded.

The mixer 1, 2 and 3 pre-selector switches are wired so that a ground is made available at additional eyelets on the relay board corresponding to the input selected. This ground is only completed when the mixer control lever switch leaves the off position. In the A-15B Console, this lever switch selects the A & B inputs to each mixer and the "C" position does not exist so the corresponding terminals on the relay boards are not used.

The relay contacts brought to the rear panel for control of remote equipment are rated at 117 v. AC 5 amps; if used to control incandescent lamp loads, it should be noted that such lamps have a cold resistance of approximately 10% of their operating value. Unless provided with current limiting, lamp loads should be limited to 40 watts per relay to avoid damage from initial current surges. The relay contacts are completely isolated from the console proper and under no circumstances should power be applied to them from within the console to avoid shock hazard from the exposed Jones-connector blades.

CIRCUIT DESCRIPTION, SPARTA AUDIO CONSOLES

GENERAL. The description to follow is generally applicable to all SPARTA consoles, mono or stereo and outlines the basic system of selecting, mixing and amplifying the usual program-sources plus the methods used to process auxiliary functions such as cue and monitor signals. Features applicable to specific consoles are then discussed elsewhere in the appropriate manual sections.

Microphone Preamplifiers. With a nominal gain of 55db. the output level from the preamp to the mixer potentiometer is typically - 10 to 0 dbm. depending, of course, on the sound level and microphone used. In a normal situation, then, the preamplifier output is at essentially the same level as the high-level input signals, resulting in approximately the same mixer-level settings for normal operation. Preamp gain can be changed to accommodate unusual situations by referring to the preamplifier circuit description.

As normally supplied by SPARTA, the input transformer is wired for use with 150/250 ohm microphones. A transformer tap is provided for easy conversion to use with 30/50 ohm microphones.

All SPARTA Audio Consoles are supplied as standard with a microphone preamplifier in the first mixer position. The preamplifiers are interchangeable with high-level input cards, however, so additional microphone

CIRCUIT DESCRIPTION, GENERAL

preamplifiers may be incorporated, or alternately, all inputs may be high-level.

High-Level Inputs are brought to the primaries of input-isolation transformers which are suitably terminated and connected directly to the proper Mixer potentiometers. The primaries are floating (ungrounded) to allow single-ended connection and also to prevent the possibility of setting up undesired ground-loops or common-mode signals via the input cables.

Mixing takes place by feeding the output of each mixer potentiometer through a high-value series resistor (10K or 27K) to a common mixing bus, which in turn leads to a mixing amplifier. The mixing amplifier, which is usually located with the line amplifier, is specifically designed to have a very low input impedance, typically 100 ohms.

Since the Mixer feed resistors are so much higher in value, the mixer amp becomes a "current sink" and responds to the current in the feed resistors, which in turn is determined by the voltage available from the Mixer pots. The output of the mixer amp, then, is proportional to the sum of the currents at its input.

CIRCUIT DESCRIPTION, GENERAL

Mixer isolation is excellent with this system since the current from each feed resistor will follow the easiest path -- obviously into the mixer amp rather than to another Mixer pot. Changing one mixer-pot, then, will have relatively little effect upon the program level coming from another mixer-pot.

There is obviously a significant loss of program power in the mixer feed resistors, but the power levels are so low that it is a simple matter to recover the loss in the mixer amplifier. Mixer amp. gain is set to restore the program to substantially the same level as originally fed to the mixer pots, with the mixer-pots at their usual operating positions, about one o'clock.

Since a "current" mixer operates from a relatively high source impedance, it allows the use of high impedance mixer-pots. And since it is not critical of the precise source impedance, there is no need to resort to the bulk and cost of precision ladder attenuators.

Output of the mixer system is then fed to the Master gain control at essentially the same level as the original high-level program material. To test the entire mixer system, a -10 or 0 dbm signal is provided at a high-level input, the appropriate mixer pot is set at the normal operating position and the signal is viewed or measured across the Master gain control.

CIRCUIT DESCRIPTION, GENERAL

The Line Amplifier provides the final amplification between the Master gain control and the line output terminals. It must therefore recover the signal loss of the Master gain control, compensate for any losses in matching or isolation pads, and provide power-gain for driving the output line at rated level.

For a rated output of 8dbm into a 600 ohm line at zero VU, several factors must be considered: A minimum of 10 dbm of additional gain, without distortion, must be available to handle program peaks (headroom). Also, the output transformer must be isolated from the line with a pad, typically 4 db, to prevent interaction with line reactances. Finally, the line amplifier output-impedance must properly match the line transformer primary so the output terminals are a true 600 ohm source.

The line transformer must then handle a nominal level of 12dbm, and 22dbm on program peaks. The line amplifier must be capable of supplying 18 dbm to the line plus the power-losses in the line pad, insertion loss in the transformer and internal loss necessary to obtain a proper impedance match. This is considered in detail in the line-amplifier section of the manual.

VU Meter. The standard VU meter contains rectifier diodes and consequently appears as a non-linear impedance to its signal source. To avoid introducing

CIRCUIT DESCRIPTION, GENERAL

distortion on the program-line, it is necessary to provide isolation between the meter and the line.

It is also necessary to attenuate the level to the meter so it can indicate 0 vu when the line is at 8dbm and finally, the attenuator must be so designed as to appear to the meter as a 3.9L ohm source to preserve the linearity of the meter indication.

This latter requirement accounts for the meter pad being a "T" configuration rather than a simple series resistor. In SPARTA consoles, the metering source is the line transformer output, ahead of the line pad, which allows an added 4 db of attenuation in the meter pad for increased isolation. A balanced "H" pad is not required since the meter need not be balanced to ground.

Cue. Common to all SPARTA consoles is a "Cue" position on each Mixer potentiometer. In the simplest case, program material from each mixer, through the cue switches and isolation resistors, is delivered to a rear-panel terminal for feed to an external cue amplifier. In more elaborate consoles, a cue level control, internal amplifier and optional-use internal speaker are provided.

Monitor. Although provisions for program-line monitoring vary in different SPARTA consoles, in all cases the source of program material is the output

CIRCUIT DESCRIPTION, GENERAL

stage of the program line amplifier. Since there are no active or non-linear components to follow, the monitor provides constant assurance of both level and quality, whereas the VU meter alone only indicates level.

CIRCUIT DESCRIPTION/MAINTENANCE

PREAMPLIFIER, 1018

The 1018 Preamplifier is supplied standard for operation with 150/250 ohm microphones and provides a nominal gain of 55db into a 600 ohm or higher load. A jumper is provided on the circuit board, either a wire or a low-value resistor, to accommodate 30/50 ohm microphones.

The 1018 Preamplifier differs from its predecessor, the 1008A, in several respects. The microphone transformer is a miniaturized PC-mounting type with extended high and low frequency response. The 1018 circuitry takes full advantage of the transformer's 80K secondary impedance to provide improved noise performance, expanded frequency response and excellent overload characteristics.

With normal microphone input levels, the output level to the mixer will be approximately 0 dbm. The maximum output level of the 1018 before clipping is in excess of 14 dbm, which assures more than adequate head-room in normal operation. In the event that microphones must be used, which provide unusually high output, a pad may be added in series with the microphone or a resistor in the 1018 may be changed in value to lower the preamp gain, as described later.

The input signal is amplified approximately 20db by the input transformer and then amplified a further 35db by transistors Q1 and Q2. The output signal from Q2 then passes through emitter-follower Q3 to provide the necessary low output impedance.

The emitter of Q2 is heavily bypassed to ground by capacitor C8; therefore the base impedance of Q2 is quite low, being essentially a forward-biased diode.

Most of the signal current from Q1 passes to the base of Q2, then, rather than through the much higher impedance of the collector resistor R3. This assures maximum current gain from Q1, although the voltage gain is relatively small.

The emitter of Q3 is not bypassed, however, so the base impedance of Q3 is relatively high compared to Q2's collector resistor R4. The signal current from Q2 must therefore cause a significant signal voltage across R4. This assures a maximum of voltage gain from Q2, and since Q3 is an emitter-follower this signal appears at the low impedance emitter of Q3.

A portion of the output signal determined by feedback attenuator R8/R9 appears at the emitter of Q1. Since Q1 and Q2 both invert the signals through them, the feed-back to the emitter of Q1 is in-phase with the signal input to the base of Q1. This constitutes negative feed-back, since the feed-back attempts to cancel the input signal. The open-loop gain (without feed-back) is extremely high, so the normal closed-loop gain is determined by the turns-ratio of the input transformer plus the ratio of R8 to R9. It can now be seen that changing the value of either R8 or R9 will change the gain of the amplifier proportionally. For example, if R9 were to be increased to 360 ohms, the voltage gain of the amplifier would decrease by 6db, since the output of the amplifier would only need to swing half as far to provide the same feed-back voltage to the emitter of Q1. Consequently, reasonable selection of gain can be obtained simply by selecting the value of R9.

The use of negative feedback to control gain via the input emitter also has the effect of raising the input impedance to Q1. This permits the use of a high-ratio

input transformer for added voltage-gain without added noise. Distortion is also lowered with negative feed-back since any difference between the input and output wave-forms appears as an error signal. Distortion in the 1018 is held well below 0.1%.

A stable operating-point, or "Q", is one of the most important characteristics of an amplifier because the maximum signal output without clipping, and therefore the headroom is determined by the average DC voltage at the emitter of Q3. The emitter can move no higher than the supply voltage and no lower than ground, so the ideal operating-point, permitting maximum dynamic range, is logically somewhere near to one-half the supply voltage.

The emitter voltage of Q3 is set by the collector voltage of Q2 and since the collector current of Q2 is also the emitter current of Q2, any change in the collector voltage of Q2 also appears as an inverted change at the emitter of Q2. The bias current for Q1 is obtained through R6 from the emitter of Q2; therefore, any change of emitter voltage at Q2 results in a corrective change of bias current to Q1. This not only provides normal operating bias for Q1, but any change at Q2 is also fed-back to Q1, as an error signal to maintain the proper operating-point.

Maintenance: From the foregoing circuit description, it can be surmised that failure of any component involved in the DC biasing of the circuit, including leaky capacitors, will cause a shift in the operating-point of Q3. Stated in a more useful manner, if the emitter of Q3 is at a reasonable voltage, then all of the components involved must be functioning normally.

During trouble-shooting most components, including the transistors, can be removed from question simply by making two DC voltage measurements: First, the supply voltage at terminal 3, and second, the voltage at the emitter of Q3. When we consider that resistors may vary 5% or 10% and individual transistor gains may vary by a factor of 2 or more, it is reasonable to expect a possible variation of $\pm 20\%$ or so in the operating point. This, then, would indicate a reasonable voltage range for the emitter of Q3 of from approximately 10.5 to 15.5 volts. In the event of catastrophic failure of any of the resistors or transistors, or of excessive leakage or shorts in any of the capacitors, it will almost invariably result in a gross shift of the operating-point towards the supply or towards ground. If the operating-point is beyond the limit given but still capable of moving further in either direction, the amplifier will still be operative; it simply will not have as much dynamic range or head room.

If the operating point is found to be correct, but the amplifier gain is abnormally high or low, (which usually would be accompanied by high distortion) it would most likely be due to either an open capacitor or a defective input transformer. Transistor failure would normally not be a factor simply because, at audio frequencies, a transistor cannot tell the difference between AC and DC, so we would look for a component which could alter the signal gain without affecting the DC operating-point. Excessive noise can be due to almost any component. The most likely suspects would be the input transistor, Q1, followed by the resistors and capacitors associated with the first stage since noise generated there would be subject to the most amplification.

CIRCUITRY DESCRIPTION/MAINTENANCE

Mixer & Line Amps 1020

The 1020 board consists of two independent amplifiers; a mixer amp and a program line amp. The mixer amp is characterized by very low input and moderate output impedances and the program line amp by high input and low output impedances.

Mixer Amplifier: The input signals to the mixer amplifier are obtained from a group of mixer potentiometers and each one must be capable of being switched or adjusted in level without affecting the level coming from the others. The mixer amplifier is specifically designed for very low input Z (100 ohms) and is supplied signal currents from the mixers through high value resistors of 10K ohms or more. Each input current, then, follows the path of least resistance into the mixer amplifier, independent of the condition of the other mixing channels, thereby providing excellent isolation between mixer channels.

With a very low input Z and high source Z , the input signals take the form of a current which is a linear function of the source voltage. The unusually low distortion characteristics accrue in part because small changes of an already low input Z have virtually no effect on the signal input currents. Obviously, the voltage attenuation of the mixer system is quite high -- it is the input current which determines the output voltage of the mixer amplifier. The output impedance is sufficiently low to serve as a voltage-source for the Master gain control. The mixer amplifier therefore operates in the

Mixer Amplifier (cont'd)

"trans-impedance" mode; that is, the output voltage is a linear function of the input current, not the input voltage. A measure of voltage gain is not appropriate unless the input voltage is applied through a series feed resistor and the measured gain will then depend on the value of this resistor as well as the amplifier gain.

Circuit Operation: The first stage of the mixer amplifier Q1, is a conventional grounded-emitter amplifier with operating bias determined by current from the collector via R3. A decrease of collector voltage will cause a decrease of base current, resulting in a decrease of collector current which tends to raise the collector voltage. R3 then, forms a negative feedback path which assures that Q1's operating-point remains within a reasonable range. Normal operation of Q1 will be obtained at any collector voltage between approximately 5 and 20 volts.

Bias resistor R3 also performs a secondary function: Since signal voltage from Q1's collector is also fed back to the base, it is a negative-feedback path to the signal, as well. An input signal current to the base of Q1 is met by an opposing signal current from R3, with the result that R3 appears to the input signal as a shunt impedance much lower than the schematic value. This contributes towards lowering the input impedance of the amplifier. The second stage Q2, is biased in the same manner as Q1 by R5. Although R5 does have the effect of lowering the input impedance of Q2, it is not nearly so effective since the voltage gain of Q2 is limited by the un-bypassed

Circuit Operation: (cont'd)

emitter resistor R8; therefore, the relative feedback signal current is much lower.

The voltage gain of Q2 is determined by the ratio of resistor R8 to the collector load impedance R7. Consider Q2 as having a typical beta of 100, and no external load on the collector. The emitter resistor R8 carries the collector current plus the base current, but since the base current is only 1% of the collector current, we can assume the emitter and base currents to be the same for all practical purposes.

The emitter is not bypassed, so a change of voltage at the base results in an equal change at the emitter. This in turn changes both emitter and collector currents by the same amount. But the collector current is flowing through a resistor, R7, which is ten times larger than R8, so it must cause ten times the voltage-change. The voltage-gain of Q2, then, must simply be the ratio of R7 to R8, or ten. In normal application, Q2 is loaded by the Master gain control (5K ohms) so the AC collector load impedance is 1.75 K ohms, instead of 2.7K resulting in a normal stage gain of approximately 6.5, or 16db. The unbypassed R8, then, forms a third negative-feedback path -- this time to fix the ac gain -- because the collector current through R8 produces an emitter voltage change which tends to cancel the input base voltage, thereby limiting the gain.

The collector voltage of Q2, like Q1, is not critical. The nominal signal level at the collector of Q2 is 0 dbm, or about 1 volt rms. If we allow for 12db of headroom, or 4 volts rms, the collector must be free to swing 12 volts peak-to-peak or 6 volts in either direction. So an operating-point between approximately 8 and 18 volts will assure normal operation.

Circuit Operation (cont'd)

The signal voltage at the emitter of Q2 is the same as at the base of Q2 and so is a second source of shunt negative feedback to the base of Q1. Only this time, the source is a low impedance (R8) permitting the feedback resistor R6 to be low, also. R6, then, is a fourth negative-feedback path and has the most significant effect in lowering the input Z of Q1.

In addition, the source for R6 is a voltage which is a fixed portion of the output voltage. Therefore, R6 also serves to set the gain of Q1.

When an input signal current is applied to Q1, the signal voltage at the emitter of Q2 can only rise to the point where the combined feedback currents from R3 and R6 approach cancellation of the input current, with the current through R6 being dominant.

Very low distortion results, typically 0.035%, since any difference of amplitude or phase between input and feedback currents appears as an error signal. The output voltage is therefore a linear reflection of the input current, which in turn is a linear function of voltage at the source end of the mixer feed resistors.

Gain of the mixer amplifier may be verified by applying an input signal current of 10 microamps through a minimum resistance of 2K ohms. Signal level at the collector of Q1 should be about 130 mv, and at the collector of Q2 nearly 850 mv with the output connected to the 5K Master gain pot. With no external load, the output should be nearer to 1.3v.

Circuit Operation (cont'd)

Do not be concerned by 10 or 20% gain variations, since many 10% resistors are used and are easily compensated for by the normal control settings.

Line Amplifier: The input stage, Q3 and Q4, is a differential comparator which performs three separate functions: First is signal amplification wherein Q3 operates in the transconductance mode; that is, the collector current is a function of base voltage. Second, a large proportion of the average dc voltage at the emitters of Q6 and Q7, which appears at the base of Q4, is compared to the base voltage of Q3 to stabilize the operating-points of the output transistors. And third, a small proportion of the output signal, which is fed back to the base of Q4, is compared to the input signal at the base of Q3, thereby setting the ac gain.

When power is first applied, C13 must be charged to one-half of the supply voltage through Q6, and to protect Q6 the charging-rate must be limited.

Q6 cannot turn on until Q5 and hence Q3 begin to conduct. But Q3 cannot conduct any faster than C6 can charge, so C6 not only filters the bias current to Q3, but also controls the charge-rate of C13.

The ideal dc operating-point for the output transistors Q6 and Q7 is one half of the supply voltage, because this is the point at which the greatest peak-to-peak output-voltage swing, or headroom, is available. When first turned on, C6 charges and the base of Q3 is brought to 40% of the supply voltage. As C13 charges, the voltage common to the emitters of Q6 and Q7 rises towards the supply. Upon reaching one-half of the supply voltage, 80% of this (or 40% of the supply voltage) reaches the base of Q4 via dc divider R16, R15,

Line Amplifier: (cont'd)

R14 and R22.

These resistors form a dc divider because C11 prevents output signal currents from reaching Q4 via R15/R14. Thus the comparator Q3/Q4 compares the dc operating-point of the output to the base voltage of Q3, which is as stable as R9, R10 and R11 will allow. The dc gain of the amplifier, then, is very nearly unity, resulting in an extremely stable operating-point.

The ac, or signal gain, is determined in very similar fashion: The output signal is taken from the load end of C13 so the feedback signal is a true representation of the line output. At very low frequencies, both amplitude and phase of the output will change due to the rising reactance of C13. This change will appear as an error-signal when compared with the input, and allows the reserve open-loop gain of the amplifier to correct the error, thereby permitting use of a capacitor of reasonable size and value while maintaining clean, undistorted response to below the audio range.

The ac feedback path is via divider R14 and R15 and gain is set by the ratio of these two resistors. The junction of R15 and R16 is at ac ground so R16 plays no part at audio frequencies. It can be seen, however, that ac gain would drop to near unity if C11 were open or removed. The ac gain is therefore set at 11, or 21 db.

The collector impedance of Q3 is so high that R13 has no effect on gain.

In the event of circuit failure, however, it serves to protect Q5 by

limiting base current. D1 provides ambient temperature compensation for

Line Amplifier (Cont'd)

Q6 and Q7, while R17, R20 and R21 provide operating bias and thermal stability. At maximum signal amplitudes Q6 and Q7 must approach saturation. Q6 can readily do so because its base current comes from Q5, and Q5's collector current is determined by its base current -- not its collector voltage. The base current to Q7, however, is dependent upon R18 and R19 and without C12 the base current would fall off as the base approached ground, resulting in clipping and/or distortion. With the junction of R18 and R19 "boot-strapped" from the output, R17 appears as a constant-current source to Q7 and the junction can be driven below ground.

R22 raises the source-impedance of the line amp, at the expense of nearly 6db of signal level, so as to provide a good match for the 60 ohm primary of the line output transformer. The transformer produces 10 db of voltage gain, which is followed by a 3 db loss in a resistive isolation pad. The rms signal voltage at the emitters of Q6 and Q7 is therefore the same as the rms voltage delivered to the external 600 ohm load.

If we assume a nominal 0 dbm voltage-level at the top of the Master gain control the 1020 line amplifier will produce 8 dbm (at 0 vu) into the output line with 13 db of gain left to recover the voltage loss in the Master gain control. This corresponds to normal operation at about the one-o'clock position.

Component failures, if they occur, will almost always result in a shift of operating-point. If the operating-points in the 1020 are normal, all of the components associated with dc operation must be normal, including transistors. So if an amplifier then has no ac gain, the logical suspects will be capacitors which may open without affecting dc operation. Capacitors C2, C8, and

Line Amplifier (cont'd)

C10 may safely be ignored at this time since they are only effective above the audio spectrum.

Noise or hiss, may be due to almost any component but these associated with Q1 or Q3 and Q4 would be most suspect since subsequent gain is the highest. Hum (120 Hz) would of course lead one to the power supply.

Distortion will be practically non-existent if normal dc and ac gain is obtained. The line amplifier, for example has an open-loop gain of more than 66 db, providing more than 45 db of feedback so that distortion is almost un-measureable. If distortion does arise, it will almost always be the result of transistor substitution.

CIRCUIT DESC./MAINTENANCE

Monitor Amplifier 1025A

The 1025 Monitor Amp provides 8 watts rms into an 8 ohm speaker load and will deliver slightly higher power into loads as low as 4 ohms. With loads higher than 8 ohms, power is limited primarily by the power-supply voltage and will be correspondingly reduced.

The output circuitry is transformerless and can be considered as a virtually true voltage source; that is, the source impedance is very low compared to the load impedance. For this reason the load should never be less than 4 ohms, and a short-circuit should be avoided at all costs.

The input impedance is quite high, 50K ohms and the AC gain is set at approximately 40 (32db) by a closed-loop feedback network. The open-loop gain is nearly 2000 which accounts in part for the typically low distortion of less than 0.5%.

DC stability (output "Q" point) is stabilized by a DC feedback loop which sets the DC gain to near-unity and samples the output-stage operating-point.

CIRCUIT DESCRIPTION: The input transistor Q1 operates in the transconductance mode (output current proportional to input voltage) with both AC and DC feedback to the emitter. Since the output stage is in-phase with the input signal, feedback to the emitter tends to cancel the input voltage and is therefore negative feedback.

The second stage Q2 operates in the trans-impedance mode by converting its base current to a rather large collector-voltage swing. The voltage gain, per se, of the 1025A takes place in this stage.

Transistors Q3 and Q4 are a complementary pair that provide current gain for driving the totem-pole output pair, Q5 and Q6. Although Q3 may appear to be providing voltage-gain, it actually is simply providing phase-inversion and base-current

drive to Q5 as a conventional Darlington driver. To do so, its CE voltage must follow that of Q2.

DC FEEDBACK: The Key to circuit understanding and easy repair lies in the feedback networks. Referring to the schematic S-14, the collector voltage of Q5 should be very near to one-half of the supply voltage, or 14 volts, to assure that the output signal voltage can swing an equal amount in both directions before clipping occurs.

The output voltage is fed via R7 and R6 to the emitter of Q1, where it is compared to the base voltage of Q1 as determined by divider R2/R3. If the average output voltage tries to change in either direction, it appears as an error signal to Q1, and therefore the output operating-point is determined almost solely by R2 and R3.

Capacitor C4 prevents output voltage changes at an audio rate from reaching Q1 via R7, so that at DC and sub-audible frequencies the gain is very near to unity, insuring that the average output-stage voltage is essentially the same as the base of Q1.

Closer examination will show that R5 will act as a divider with R6 and R7 so that the emitter voltage of Q1 would be less than the output voltage. Because of this attenuation, plus the EB drop of Q1, the base voltage of Q1 is set slightly higher than one-half of the supply.

In the event of circuit failure, the first step is to measure the collector voltage of Q5. If it is correct, then all transistors and resistors are normal since neither can tell the difference between DC and audio AC!

AC FEEDBACK: The AC gain is determined by a secondary feedback network in a manner similar to the DC case. The output voltage from terminal 3 is fed back to

Q1 via R5. Since the junction of R6 and R7 is AC bypassed to ground, R5 and R6 comprise an AC voltage divider. The AC output voltage, then, is allowed to be higher than the input by the ratio of R5 to R6. Since R5 is so much higher than R6 plus R7, it has little effect upon the DC operating point.

By taking the AC feedback from the load end of C6, the full open-loop gain of the amplifier is used to correct for amplitude loss and phase-shift at the lowest frequencies. This allows extended low-frequency response with a reasonable value for C6.

BIAS: Diode D1 and resistor R8 comprise a bias network to assure that Q3 to Q6 are always conducting so as to avoid "crossover" distortion. The quiescent current of the 1025 is determined primarily by the idling current of Q5 and Q6, and should normally not exceed 10 or 12 ma.

Since all transistors are silicon, if the quiescent current is too high diode D1 should immediately be suspect. If the operating-point is normal the problem can be localized by shorting the bases of Q3 and Q4 together. The idling current should drop sharply, thereby eliminating Q3 to Q6 as possible causes.



WARRANTY

SPARTA ELECTRONIC CORPORATION (SPARTA") expressly warrants products manufactured by it and bearing SPARTA model numbers to be free from defective material and factory workmanship.

THE FOREGOING EXPRESS WARRANTY IS IN LIEU OF ALL OTHER WARRANTIES, EXPRESS OR IMPLIED, IT BEING EXPRESSLY UNDERSTOOD AND AGREED THAT SPARTA DOES NOT WARRANTY EITHER THE MERCHANTABILITY OF ITS PRODUCTS OR THEIR FITNESS FOR A PARTICULAR PURPOSE.

The obligation of SPARTA under the foregoing express warranty is limited to repairing any warranted product which upon SPARTA's examination proves to be subject to defective material and/or factory workmanship, when such product is returned to our factory, transportation prepaid by the purchaser, within one year from the date of original purchase from SPARTA. Under no circumstances shall a breach of any warranty by SPARTA subject SPARTA to any claim for consequential damages, the purchaser expressly assuming all risk of such consequential damages. In the case of any breach of any warranty, the liability of SPARTA shall not under any circumstances exceed the cost of repair or replacement of the defective product.

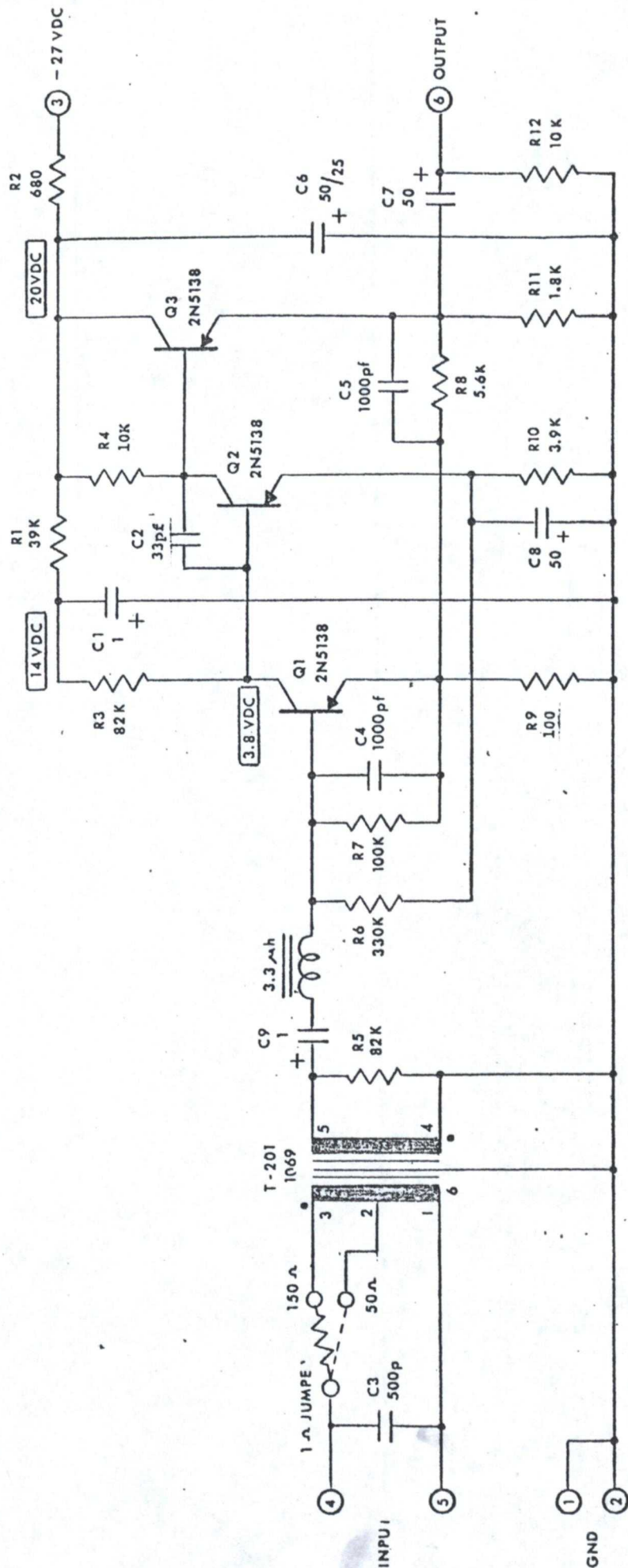
High voltage transformers, modulation transformers, reactors and filter chokes carry an extended warranty of 50% of the replacement cost being allowed should failure occur during the second year.

The foregoing express warranty does not apply to any products manufactured by SPARTA that have been repaired, worked upon or altered by persons not authorized by SPARTA, or that have been subject to misuse, negligence or accident, or the serial number of which has been altered, effaced or removed; neither does the foregoing express warranty apply to any products of SPARTA that have been connected, installed, used or adjusted otherwise than in accordance with the instructions furnished by SPARTA. Accessories, allied equipment, and components supplied, but not manufactured by SPARTA are not warranted, either expressly or impliedly, by SPARTA, and shall carry only such warranty, if any, as is made by the manufacturer of such product.

The foregoing warranty shall be void if SPARTA shall inspect any product and find it to have been modified, improperly installed or misused.

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SPARTA reserves the right to make changes in design and improvements upon its products without assuming any obligation to install the same upon any of its products theretofore manufactured.



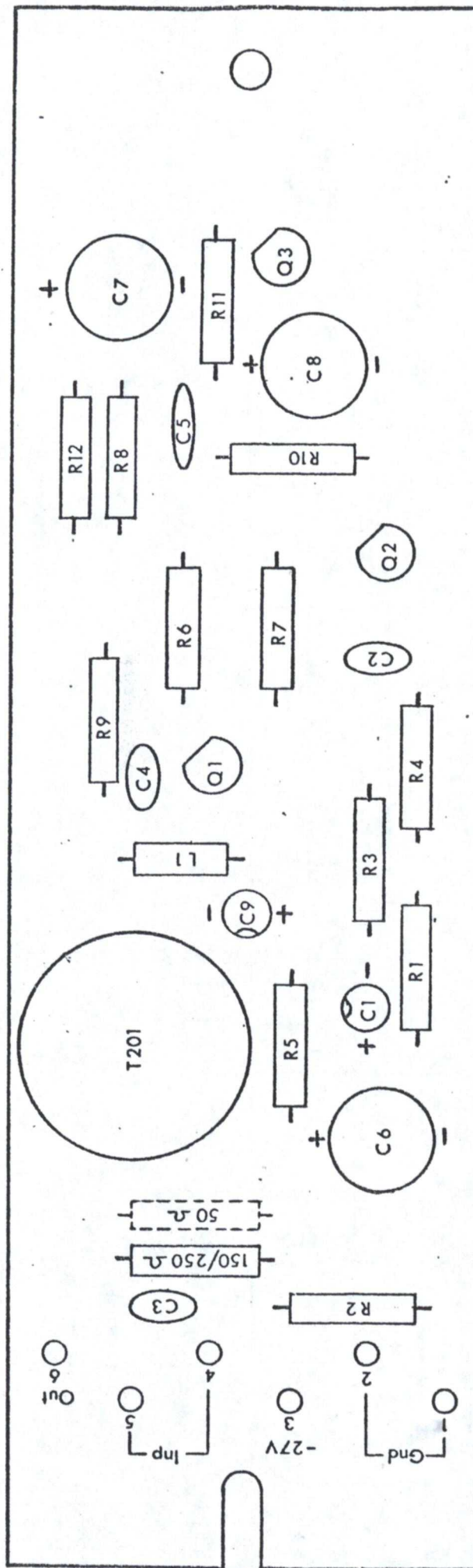
1008A-5	1018	FUNCTION
1	4	INPUT
2	5	INPUT
3	1	GND
4	2	GND
5	-	N.C.
6	6	OUTPUT
7	3	-27VDC

SPARTA ELECTRONIC CORPORATION			
1018 MICROPHONE PREAMP			
(401 BOARD)			
DRAWN	CHECKED	DATE	NUMBER
SMU	RKO	8-28-69	S-11-G

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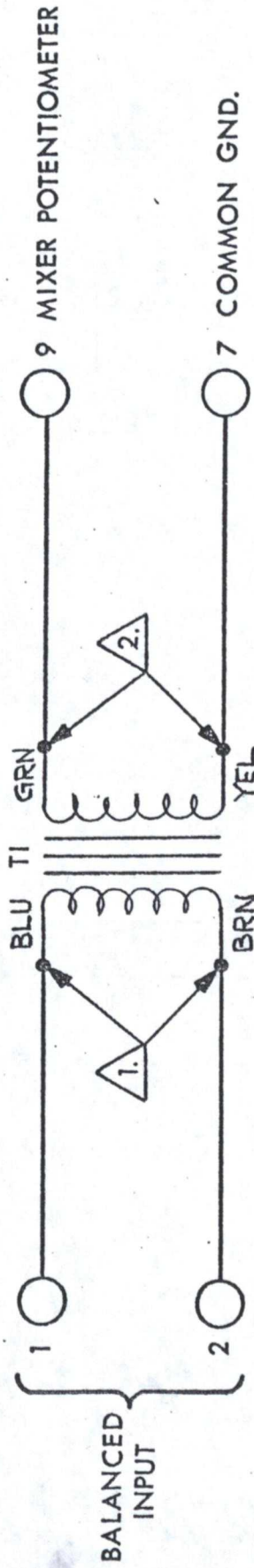
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ECR643
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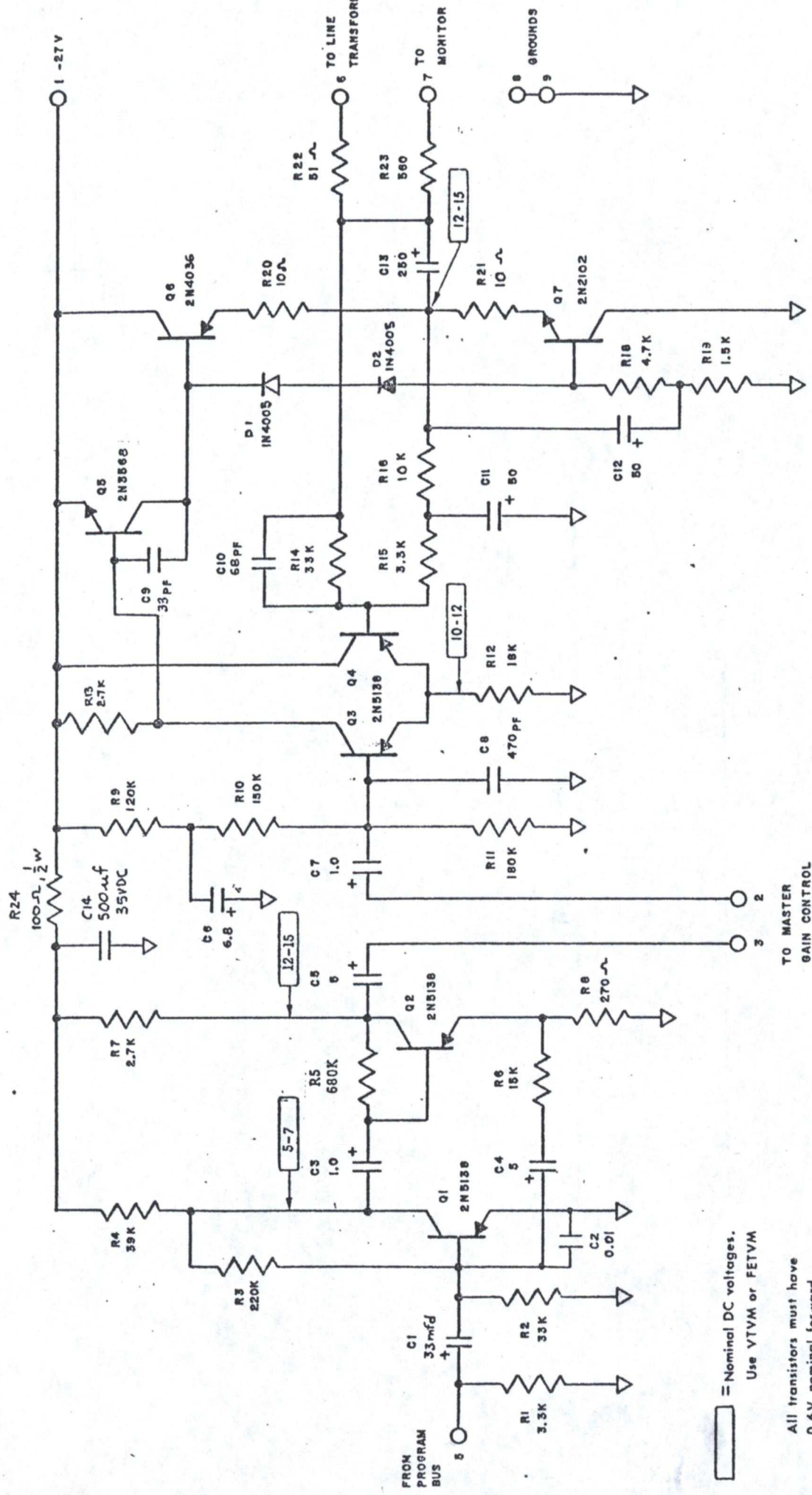
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- TI.
- SPARTA 23W7, 10K ohms, 1:1 TURNS RATIO.
OPTIONAL, 600 ohms, 1:1 TURNS RATIO.
- OPTIONAL 620 ohm TERMINATION RESISTOR,
USE WITH 10K BRIDGING TRANSFORMER ONLY.
- TERMINATING RESISTOR, 620 ohms, REQUIRED
WITH 600 ohm TRANSFORMER ONLY.

SPARTA ELECTRONIC CORPORATION			
1019 LINE TRANSFORMER ASSY HIGH-LEVEL INPUT, 065-4010			
DRAWN	CHECKED	DATE	NUMBER
ZJS.	RKO	7-23-71	S-137A



[] = Nominal DC voltages.
 Use VTVM or FETVM

All transistors must have
 0.6V nominal forward
 emitter-to-base bias.
 ECR 580 R17 was 68Ω
 ECR 487 ADD R24 & C14
 ECR 278

ECR 199, C9 was 10pF
 ECR 177

13 Oct 70 ECR 150

15 JULY 70: ECR 114, Q5 WAS 2N3568

12 FEB 70: ECR 52

6 FEB 70: ECR 46

12 FEB 70: ECR 46

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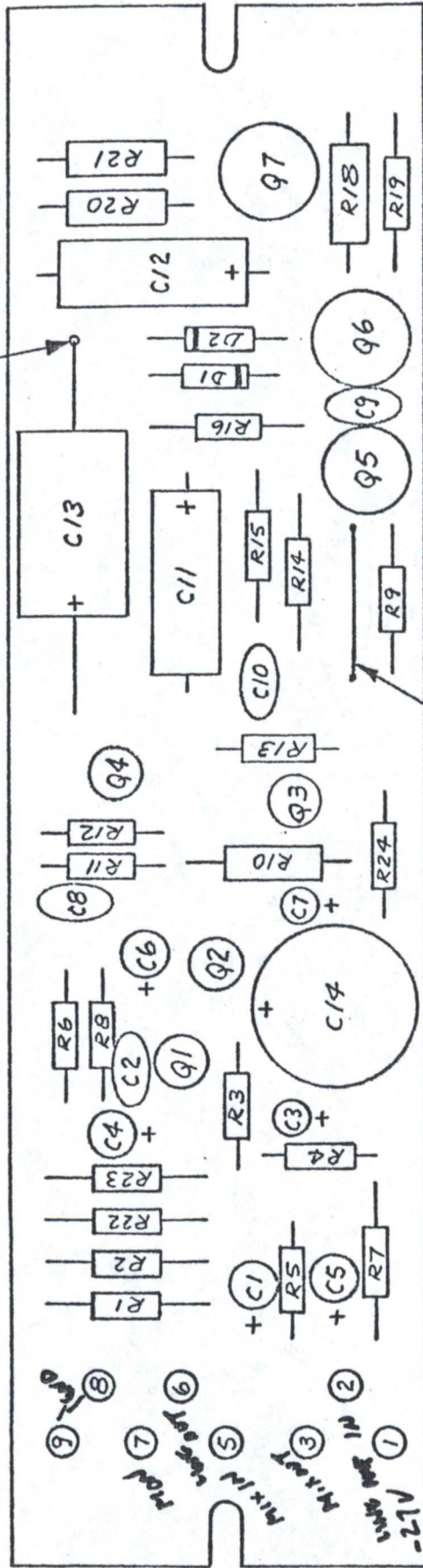
SPARTA
 ELECTRONIC CORPORATION
 SACRAMENTO, CALIFORNIA

TITLE

1020
PROGRAM LINE AMP
& MIXER AMP

DRWN. 5776	DATE 4-15-69	SHT OF 1	DWG. NO. S-2N
APPD.	REV. 24 FEB 73		

-12 TO -15 VDC
BALANCE TEST
($\frac{1}{2} V_{CC}$)



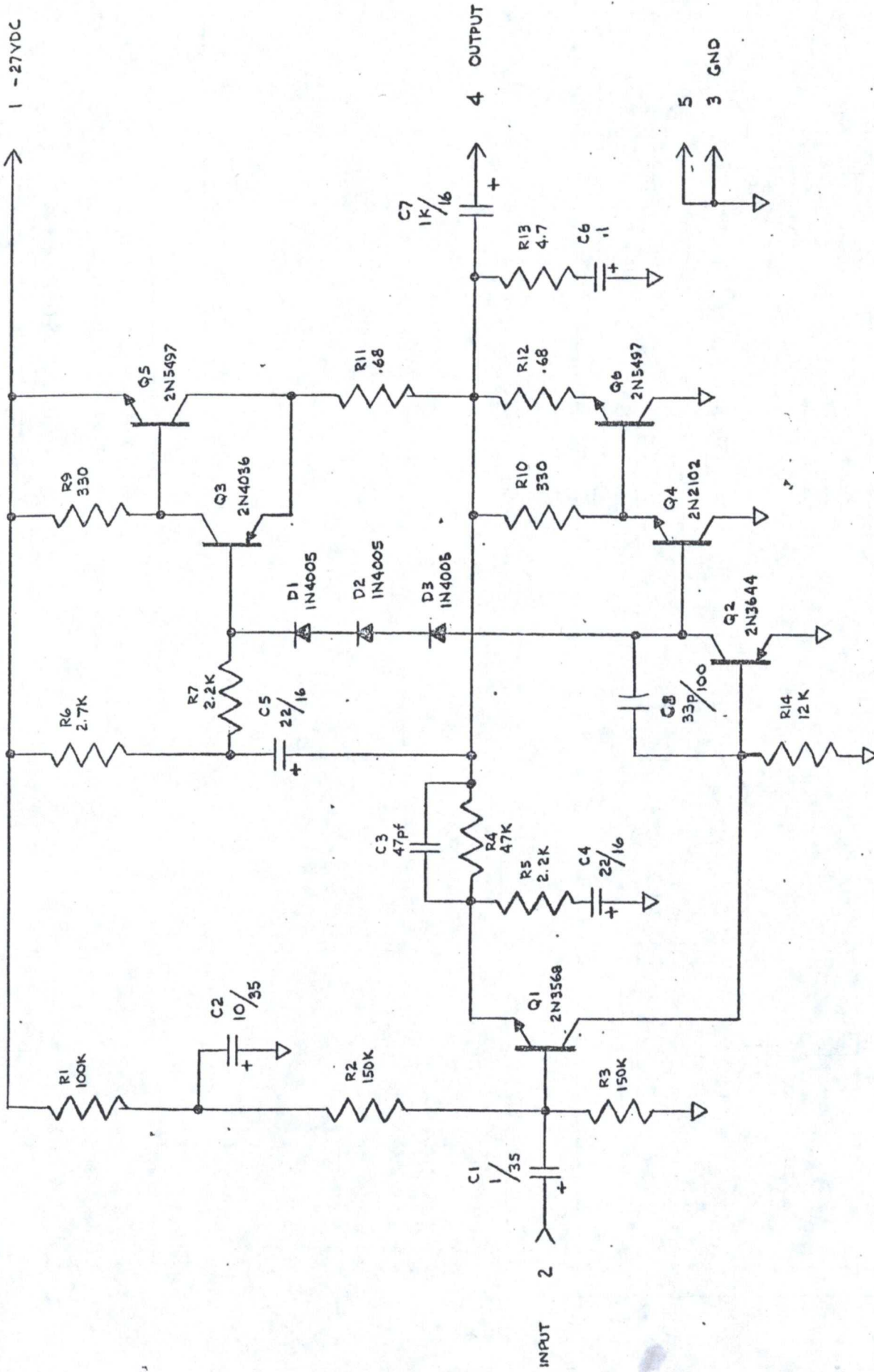
JUMPER

- ① -27 VDC
- ② LINE AMP IN
- ③ MIX AMP OUT
- ④ MIX AMP IN
- ⑤ LINE AMP OUT
- ⑥ MONITOR
- ⑦ GND
- ⑧
- ⑨

REFER TO SCHEMATIC S-2K

SPARTA ELECTRONIC CORPORATION		TITLE 1020 MIX/LINE AMP	
SACRAMENTO, CALIFORNIA 95828 A DIVISION OF COMPUTER ELECTRONIC CORPORATION		P.C. BOARD #065-3010 B	
DYN SPILL	DATE 7/1/73	SCALE 	SHIT OK
APPD 	DATE 	DATE 	P. 3/B

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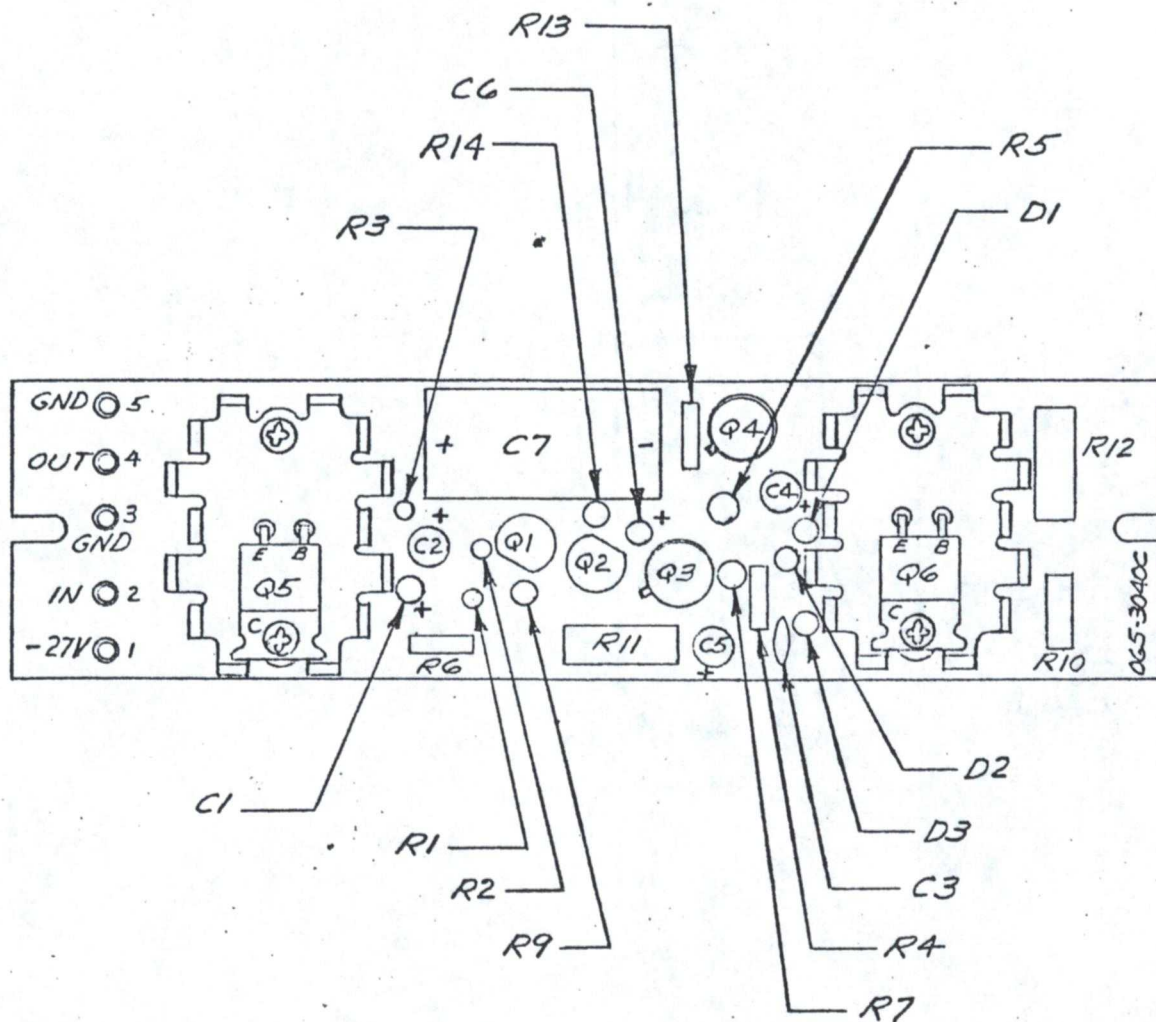
SACRAMENTO, CALIFORNIA 95828
A DIVISION OF SPARTAN INDUSTRIES CORPORATION


TITLE 1025A
MONITOR / CUE
AMPLIFIER

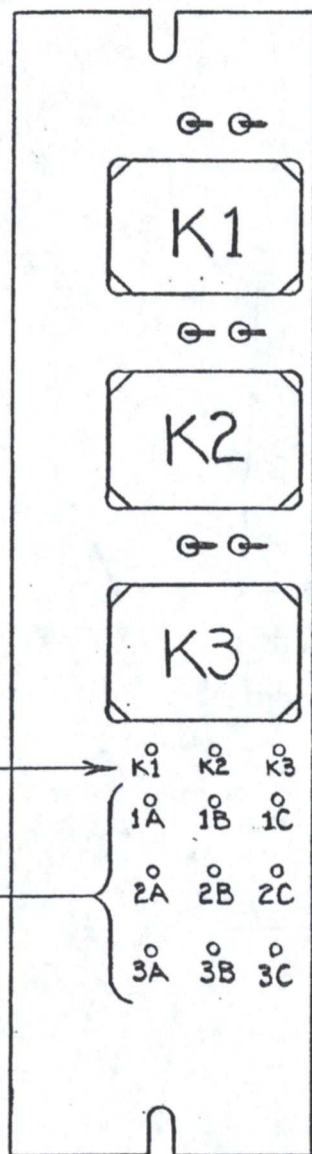
SHEET 1 OF 1
DWG NO. S-103F

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SEE ECR 1041
ECR 681-682 REDRAWN
ECR 7995

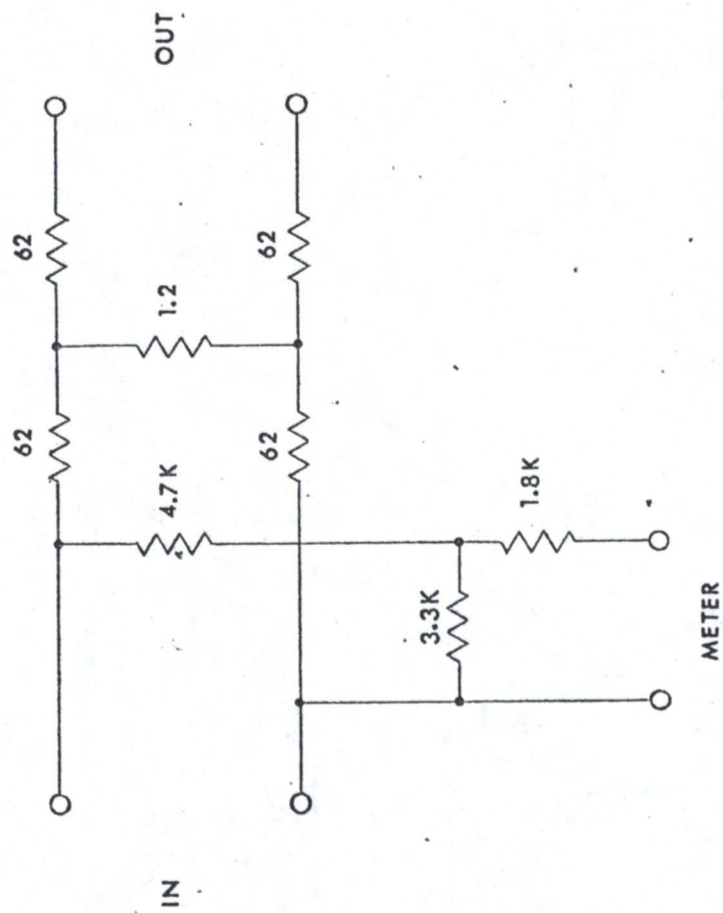


 SPARTA ELECTRONIC CORPORATION SACRAMENTO, CALIFORNIA 95828 <small>A DIVISION OF COMPUTER EQUIPMENT CORPORATION</small>		TITLE	
		1025 PICTORIAL P.C. BOARD	
DWN R.A.G.	DATE 7-21-75	SCALE FULL	SHT 1
APPD L.W.E.	DATE 7-21-75	of 1	DWG NO. P-49




NOTE: "C" TERMINALS NOT USED IN A-15B

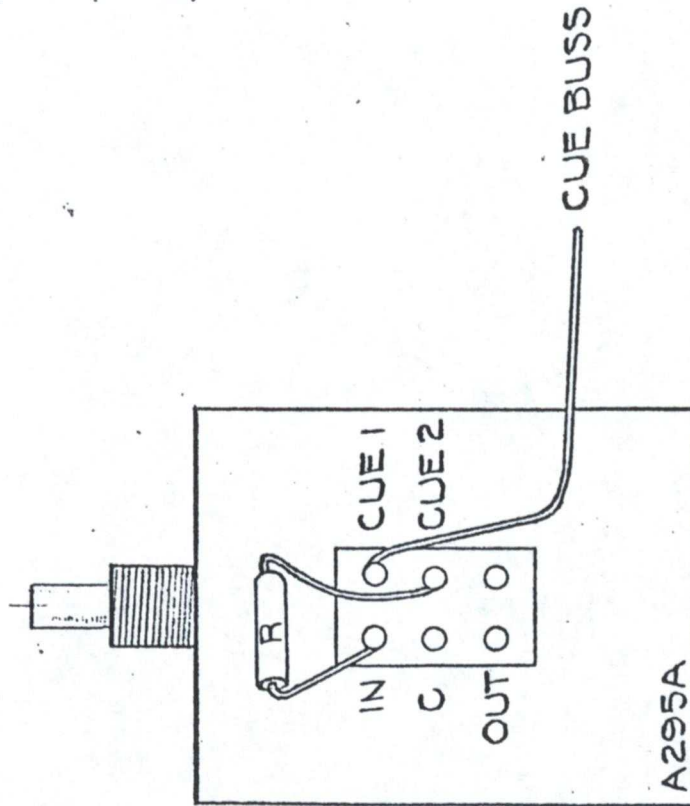
 SPARTA ELECTRONIC CORPORATION SACRAMENTO, CALIFORNIA 95828 <small>A DIVISION OF COMPUTER EQUIPMENT CORPORATION</small>			TITLE	
			1027 MUTE RELAY ASSY	
DWN B. SCUDDER	DATE 12-1-70	SCALE 1/1	SHT 1	DWG NO.
APPD R. D. G. A. S.	DATE		OF 1	P-14



Resistors $\frac{1}{2}$ w 5%

 SPARTA ELECTRONIC CORPORATION SACRAMENTO, CALIFORNIA 95828 <small>A DIVISION OF COMPUTER EQUIPMENT CORPORATION</small>		TITLE		901 METER PAD	
		DWN	SMIL	DATE	28 OCT 70
APPD	PK	DATE		SHT	OF
				DWG NO.	S-108 A

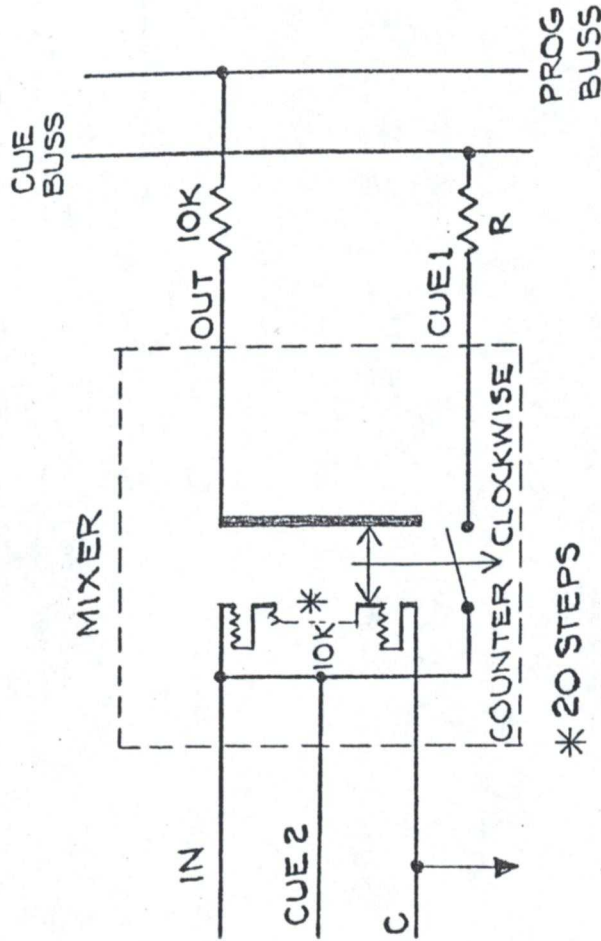
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TIEPOINT

SHOWS USE OF TIEPOINT
ON SIDE OF CASE.

R = 10K FOR A-20B
R = 33K FOR A-15B



*20 STEPS

WIRING CHANGES WHEN
STEPPING MIXERS ARE
USED INSTEAD OF
COMPOSITION TYPE.

		TITLE PRECISION STEP ATTENUATOR MONO	
SACRAMENTO, CALIFORNIA 95828		SHT 1 OF 1	DWG NO. P-52A
DWN B. SCUDDER	DATE 6-7-76	SCALE	
CHKD I. T.	DATE 7-7-76		
APPD	DATE		

